

Power Angle Small-Signal Stability Analysis of Grid-Forming Wind Turbine Inverter Based on VSM Control

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Abstract—This paper introduces a virtual synchronous machine (VSM) control scheme which is based on a minimized emulation of the model of a synchronous generator (SG) for a grid-forming wind turbine (WT) inverter. Based on this VSM control scheme, state-space representation and block diagram of the small-signal model for the VSM-controlled grid-forming inverter connected to an infinite bus are derived, which are used for small-signal stability analysis of the power angle in the VSM control scheme. This power angle small-signal stability (PAS) analysis is proposed as a simpler way for analyzing the influence on the rotor angle stability of power system from large share of VSM-controlled grid-forming inverters. Influence of parameters in the power loop of the control scheme on the PAS is investigated by analyzing the eigenvalue trajectories of the state matrix.

Keywords—grid-forming WT inverter, virtual synchronous machine (VSM) control, rotor angle stability, power angle small-signal stability (PAS), eigenvalue trajectory

I. INTRODUCTION

Synchronous generators (SGs) are the main power sources in our traditional power system today. Due to the coupling of their mechanical rotating speed and the frequency of the power grid, their huge inertia makes it difficult to have a large rate of change of frequency (RoCoF) when there is a large power imbalance between generation and load (resulting in a frequency event). Furthermore, their power input can be regulated automatically to counteract the power imbalance, which stabilizes frequency back to a steady state. These two aspects help to maintain the frequency stability of the power system.

However, for state of the art wind turbines (WTs), namely type-3 WT or type-4 WT, either with optimal speed control for maximum power point tracking (MPPT) or with back-to-back converters fully interfaced with the power grid, make their mechanical rotating speed decoupled from the frequency of the grid. As a result, the inertia of their rotating masses will not help to limit the RoCoF, as an SG does, when there is a frequency event. Besides, another significant difference between a WT and an SG is that the power source for a WT is not controllable, which makes it difficult for a WT to change its power output as demanded. These two differences bring a big challenge for the frequency stability of our power system with more and more wind power being integrated into our power grid nowadays.

To avoid this problem, a straightforward idea has been controlling a WT to behave in the same or similar way as an SG. This is how the concept of virtual synchronous machine (VSM) control comes from [1]–[4]. Specifically, VSM control is one category of control schemes applied to converters, which enables WTs to perform similar frequency control as SGs, by adding a SG model in the control schemes.

Considering the big differences between a converter and an SG in structures and characteristics, it is feasible only to emulate the desirable properties of an SG rather than also to include the undesirable ones, like complex electromagnetic dynamics. In this way, the control scheme will also be simpler, which helps to keep the advantages of converter control, like fast response and flexibility. Hence, it is considered as an objective in this study to get a minimized emulation of the SG model for the VSM control scheme, to simplify the control scheme as much as possible while keeping qualified frequency control capability from the WT. According to this motivation, a simplified VSM control scheme is proposed [5], which is also specially designed for WT applications.

As stability analysis is very important for a control system, it is essential to analyze the stability and design the parameters of our proposed VSM control scheme, which is the main topic of this paper. To get started, this paper focuses on the small-signal stability of the power angle in the power loop of the VSM control scheme. Especially, it is another goal in this paper to have a simple and practical analysis with focus on the outer power loop only, considering the different bandwidths of inner and outer loops. Moreover, state space representation and eigenvalue sensitivity analysis are used for easiness of parameter design.

On this topic, there has been relevant research. There is small-signal stability analysis carried out using transfer functions and Bode diagrams [6]–[10]. There are publications mentioning small-signal stability but with other focuses, like synchronous frequency resonance (SFR) [6], power oscillation and suppression [7]; and some of them do not include power angle [10]–[12] or parameter design [12][13]. There are some papers most relevant with small-signal stability analysis including power angle as a state variable [13]–[24]. However, a detailed state space modeling of the whole converter control scheme and electric circuits is used in these papers, some with more than ten state variables, which is opposite to the goal of simplification in this paper. Indeed, there are some simpler representations [25][26], but they do not focus on the small-signal stability analysis and parameter design of the VSM-controlled inverter itself. Last but not the least, all the previous studies are based on VSM

This work has received funding from the European Union's Horizon 2020 research and innovation program under agreement No. 727680 (TotalControl).

This work has also received funding from project PowerKey (EUDP Project No. 12558).

control schemes specific to those studies, like synchronverter [10], [12], [16]–[19], schemes developed by SINTEF [20]–[24], Osaka University [11], Kawasaki Technology Co. [24] and others [25]. Therefore, it is also essential to analyze the small-signal stability of the proposed VSM control scheme, especially with the focus and goal mentioned above, which has not been thoroughly investigated before in the literature.

The rest of paper is organized as follows. Section II gives an introduction of the proposed VSM control scheme, of which small-signal stability analysis of the power angle and parameter design is illustrated in detail in Section III, before concluding in Section IV.

II. PROPOSED VSM CONTROL SCHEME

The motivation to propose a different VSM control scheme from those in the literature considers three aspects. Firstly, this scheme is specially designed for WTs, where type-4 WT is focused in our research. That is to say, special structure of WTs and specific requests from grid codes for wind power need to be considered and are adopted in the scheme. Secondly, this scheme is applied only for equipping WTs with frequency control capability, namely frequency containment reserve (FCR) [27]. Hence, voltage control capability is not required and optimized in the design of the scheme. Thirdly, this scheme is designed to give a minimized emulation of the SG model, which is supposed to guarantee qualified frequency control capability for WTs and meanwhile reduce undesired characteristics of SGs as much as possible.

The main blocks of the proposed control scheme are introduced briefly as follows.

A. Swing Equation

The equation representing the mechanical motion of an SG [28] is

$$\frac{2H}{\omega_n} \frac{d^2\delta}{dt^2} = T_m - T_e - \frac{D}{\omega_n} \frac{d\delta}{dt} \quad (1)$$

where

- H = inertia constant in $MW \cdot s / MVA$
- ω_n = rated angular velocity in electrical rad / s
- δ = angular position in electrical radians
- t = time in s
- T_m = mechanical torque in pu
- T_e = electromagnetic torque in pu
- D = damping factor in pu torque/pu speed deviation

It is referred to as the swing equation as it represents swings in rotor angle δ during disturbances. For analysis for its dynamics, (1) is expressed in the state-space form, which consists of two first-order differential equations [28], becoming

$$\frac{d\Delta\omega_r}{dt} = \frac{1}{2H} (T_m - T_e - D\Delta\omega_r) \quad (2)$$

$$\frac{d\delta}{dt} = \omega_n \Delta\omega_r \quad (3)$$

where

- ω_r = angular velocity in electrical rad / s
- $\Delta\omega_r$ = deviation of angular velocity in pu
- $= (\omega_r - \omega_n) / \omega_n$

From (2) it is easy to find that a big inertia (reflected by the value of H) helps to limit the value of $d\Delta\omega_r/dt$, which is equivalent to RoCoF. This is how an SG helps to keep the frequency stability by avoiding a large RoCoF, and this is the very reason that a VSM control scheme needs to include the swing equation to emulate the inertial response. A swing equation branch is based on (2) and (3) in the proposed VSM control scheme.

B. Governor

The governor for an SG with speed-droop characteristic is characterized as a proportional controller with a gain of $1/R$, shown in Fig. 1 below [28].

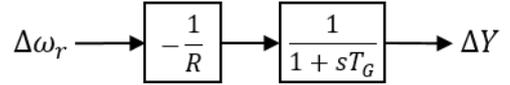


Fig. 1. Block diagram of a speed governor with droop

The parameter R , referred to as speed regulation or droop, determines the steady-state speed versus load characteristic of the SG. It is equal to the ratio of speed deviation ($\Delta\omega_r$) or frequency deviation (Δf) to change in valve/gate position (ΔY) or power output (ΔP). It is the governor that regulates the power output of SG according to the change of grid frequency and supports the grid to bring the frequency back to a new steady-state value during the FCR process.

Inspired by this, a governor branch is included in the proposed VSM control scheme, of which a droop coefficient enables the WT to have the same frequency control capability as an SG does. More importantly, similar to the right block in Fig. 1, a time delay block is also included in the governor branch of the proposed VSM control scheme, to represent the response time of different components in frequency control scheme of the WT, like pitch control, speed control or energy storage. This makes the proposed VSM control scheme specially designed for WT applications.

C. Reference Voltage Vector

The proposed VSM control scheme consists of three cascaded control loops: power loop, voltage loop and current loop. Power loop is the outermost one, voltage loop in the middle, and current loop is innermost.

The power loop generates a reference voltage vector to the voltage loop, which consists of two components: magnitude reference and phase angle reference. The phase angle reference is the power angle δ calculated after the swing equation branch. Considering the research question of frequency control and goal of qualified simplicity in this work, the magnitude reference is simply set to the reference value of voltage at point of common coupling (PCC).

D. Inner Control Loops

For the inner voltage control loop and current control loop, proportional-resonant (PR) controllers are used considering their better transient performance, limited total harmonics distortion (THD) and ease of implementation without dq transformation, compared with proportional-integral (PI) controllers [29].

In summary, the block diagram of the proposed VSM control scheme is shown in Fig. 2 below. In the governor

This is of the form $\dot{\mathbf{x}} = \mathbf{A}\mathbf{x} + \mathbf{b}u$. The elements of state matrix \mathbf{A} are seen to be dependent on system parameters X , H , D , D_r , T_g , and initial operation condition represented by E' and δ_0 . The block diagram representation is shown in Fig. 5.

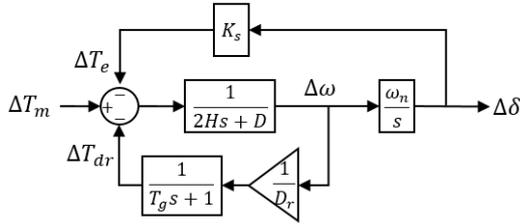


Fig. 5 Block diagram of a single-VSM infinite bus system

C. Verification

To test the correctness of the derived PAS model, differences of time-domain simulation results between the PAS model and a detailed model, which consists of a VSM-controlled inverter with PWM switching connected to an infinite bus are compared. Both models are built in MATLAB Simulink.

The PAS model is built as the block diagram shown in Fig. 5, with the parameter values in TABLE I.

The circuit of the detailed model is shown in Fig. 2, in which the grid is modeled by a voltage source. In this model, power is used as input instead of torque. The values of parameters are shown in TABLE II.

In the simulations, at $t=1s$ the mechanical torque is dropped by 0.5 pu or mechanical power by 5000 W, and the response of $\Delta\omega$ is recorded and compared. The results are shown in Fig. 6.

From the comparison, we can see these two models match very well in the first drop and recovery process of the angular speed. The only big difference is that the detailed model has a bigger overshoot, but this overshoot is relatively small compared with the nadir of the whole process. Considering that the inner voltage and current control loops and PWM of the inverter have been neglected, this PAS model gives a satisfying representation of the whole system.

Therefore, this PAS model provides a simpler way for focusing on the power loop analysis and PAS of the inverter. This will be especially helpful for analyzing the rotor angle stability of the power system in the future when large share of grid-forming inverters are integrated to the power system.

TABLE I. PARAMETERS OF THE PAS MODEL

Parameter	Value
Synchronizing torque coefficient, K_s	4.3522
Rated electrical angular speed, ω_n	314 rad/s
Inertia constant, H	0.1775 W · s / VA
Damping coefficient, D	30
Droop, D_r	0.04
Response time, T_g	0.05

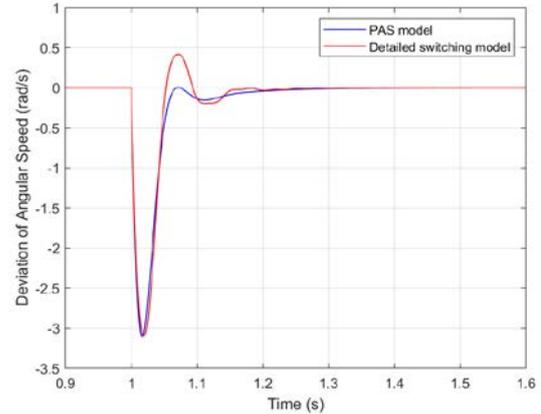


Fig. 6 Verification of the PAS model

D. Influence of Parameters on Stability

In this section the influence of parameters H , D , D_r , T_g on the PAS of the system is investigated. These parameters are investigated separately by varying the investigated parameter in a reasonable range while keeping other parameters' values fixed, equal to the values used in TABLE I. The varying range for each investigated parameter is set by decreasing and increasing certain percentages of the base value listed in TABLE I. The certain percentages are different for each investigated parameter, considering practical limits in reality.

1) Inertia constant H

The calculated base value of inertia constant H is 0.1775. Varying H from 0.1 to 0.5 and plotting the eigenvalue trajectories of the state matrix, the results shown in Fig. 7 are obtained.

From the result we can see there are three eigenvalues, as the system is a third-order system shown in (15). These two conjugated eigenvalues can be referred to as λ_1 , λ_2 and the third one λ_3 , same as below. The direction of the arrow

TABLE II. PARAMETERS OF THE DETAILED MODEL

Parameter	Value	Parameter	Value
Rated voltage, $V_{ref, ll, rms}$	400 V	Filter capacitance, C_f	1 μ F
Grid voltage, $V_{g, ll, rms}$	400 V	Grid inductance, L_g	0.01 H
Voltage base, V_b	400 V	Moment of inertia, J	0.036 $kg \cdot m^2$
DC-link voltage, V_{DC}	800 V	Damping coefficient, D	1273.9 $N \cdot m \cdot s$
Rated active power, P_{ref}	10 kW	Droop, D_r	0.04
Power base, S_b	10 kVA	Response time, T_g	0.05 s
Rated grid frequency, f_n	50 Hz	Voltage controller proportional gain, K_{pv}	0.1
Switching frequency, f_{sw}	10 kHz	Voltage controller resonant gain, K_{Rv}	500
Sampling frequency, f_s	10 kHz	Current controller proportional gain, K_{pi}	4.36
Filter inductance, L_f	1.5 mH		

represents the increase of the investigated parameter.

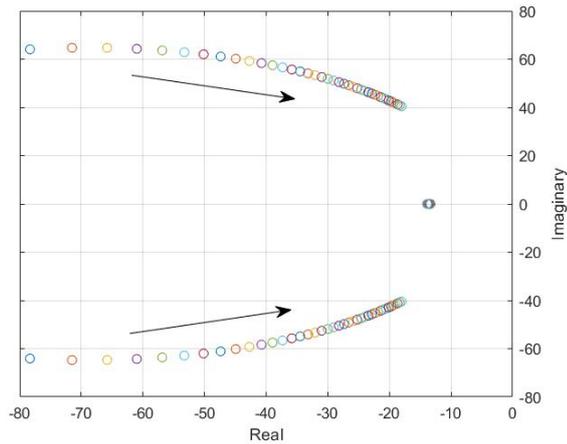


Fig. 7 Eigenvalue trajectories by varying inertia constant H

From the figure, it can be found that inertia constant H has little influence on λ_3 , while makes λ_1, λ_2 move towards the imaginary axis. This means the PAS margin is reduced when increasing H . This is physically reasonable because a bigger H means the VSM responds slowly to the torque imbalance. This means a longer dynamic process, a longer time to stabilize, and always accompanied by a larger overshoot.

However, it is also intuitive that a larger H is better for the considered grid-forming inverter from the perspective of inertia response, which is also one important aim of utilizing VSM control. A larger H helps reducing the RoCoF and partly improving the nadir of frequency (taking a frequency drop case as an example), which is consistent with the aim of frequency control by implementing VSM control.

Therefore, a compromise needs to be achieved between these two aspects. Moreover, the exact value of H will depend, among others, on the grid code requirements regarding frequency control, while it is also influenced by design choices such as the converter rating. However, the relationship between them is worth being investigated in the future.

2) Damping coefficient D

The calculated base value of the damping coefficient D is 30. Varying D from 10 to 100 and plotting the eigenvalue trajectories of the state matrix, the results shown in Fig. 8 are obtained.

From the figure, it can be seen that there is a range of D that makes the system stable and there is a range of D that makes the system unstable. Easily it can be found out that the system is stable when D is between 10 and 53; the system is unstable when D is between 54 and 100. These two cases are discussed separately below.

In the stable range, namely D is varying from 10 to 53, it can be concluded that damping coefficient D has very little influence on λ_3 , slightly making it move closer to the imaginary axis by increasing D . On the other hand, D has much influence on λ_1 and λ_2 , making them move far away from the imaginary axis.

In this range, λ_3 is the dominant eigenvalue as it is closest to the imaginary axis. As it is not changing much in this range and the system is stable, the change of performance of

the system mainly is determined by λ_1 and λ_2 when varying the value of D . From the result, we can see the performance is improved a lot. This can be explained considering these two conjugated eigenvalues represent periodical oscillating components in the system responses. When these two eigenvalues are moving leftwards and their imaginary parts are getting smaller, it means that the oscillations in the system responses are more quickly damped, in both time and magnitude, which is desirable.

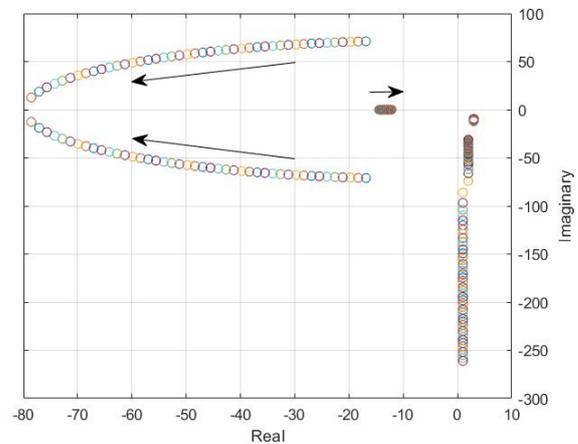


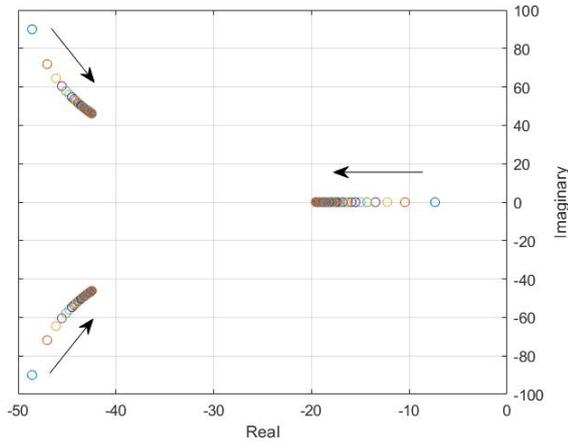
Fig. 8 Eigenvalue trajectories by varying damping coefficient D

In the unstable range, the system keeps unstable when increasing D from 54 to 100. In summary, there is a certain range of D to make the system stable. Therefore, if designing the damping coefficient D only from stability perspective, firstly, we need to find the range of D to keep the system stable; secondly, in this range, its value is supposed to be as large as possible after considering a proper safety margin.

However, the overall design of D also needs to consider the positive effects of a smaller value of D . A smaller value means less damped system responses, like larger overshoots. Although larger overshoots are not desirable generally from a stability perspective, a larger overshoot of the active power actually is desirable from the perspective of inertia response and frequency control. It is the immediate and large active power input after the frequency event that enables VSM control to equip a WT with frequency control capability. Therefore, a trade-off needs to be carefully considered between these two aspects.

3) Droop D_r

The calculated base value of the droop D_r is 4%. Varying D_r from 0.01 to 1 and plotting the eigenvalue trajectories of the state matrix, the results shown in Fig. 9 are obtained.

Fig. 9 Eigenvalue trajectories by varying droop D_r ,

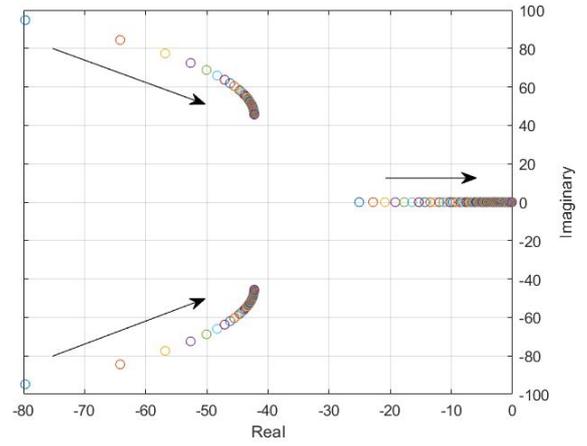
From the figure, we can see that D_r has some influence on λ_3 . As the range considered almost covers the entire possible scope of varying the droop, it can be seen that λ_3 is always the dominant eigenvalue in this range. Therefore, the stability of the system is mainly determined by the change of λ_3 . That is to say, the stability is improved when the droop is increased. This is physically reasonable because a bigger droop means larger amount of extra power is provided by the VSM to compensate the power imbalance, which is more helpful to maintain the frequency stability by bringing the frequency back to a closer steady state to the rated value.

At the same time considering the change of λ_1 and λ_2 , in the process of improving stability by increasing the droop, the magnitude of oscillations of the system response is also reduced. However, the droop cannot be increased as much as we want just to improve the stability, because it is constraint by the capability of the WT to provide or absorb extra power, also it is related with the rating of the inverter and the requirement of grid codes for frequency control capability. Probably stability issue is less important compared with these aspects. Initially and generally, it is reasonable to refer to the practical settings of SGs for the value of the droop, for instance, 4% [28].

4) Response time

Here the response time T_g represents the time needed to generate or absorb extra power to compensate the power imbalance for frequency control. The base value selected is 0.05. Varying T_g from 0.01 to 10 and plotting the eigenvalue trajectories of the state matrix, the results shown in Fig. 10 are obtained.

From the figure, we can see that the response time also has much influence on λ_3 . Summarizing the influence on λ_3 of these four parameters, it is obvious that, basically λ_3 is only influenced by the droop D_r and the response time T_g . This is because this eigenvalue λ_3 is produced by including the governor branch in the control scheme. This can be easily proved by calculating the eigenvalues for the system with a SG only represented by its swing equation. In this case, there are only two conjugated eigenvalues, which are equivalent to λ_1 and λ_2 in this VSM case. Hence, λ_3 is only influenced by the two parameters that are forming the governor branch.

Fig. 10 Eigenvalue trajectories by varying response time T_g

From Fig. 10, it is easy to conclude that the stability of the system is worsen when increasing T_g . Therefore, from the perspective of stability, it is better to equip WTs with a quicker responding power source for frequency control capability.

What needs to be noticed from Fig. 10 is that, the system is still stable even when T_g is 10, in which case λ_3 is closest to the origin. Considering that a response time of 10 seconds is already beyond the scope of fast primary frequency control requirement, which is recently proposed by EirGrid, therefore, discussion of T_g larger than 10 is beyond the scope of this study.

IV. CONCLUSION

This paper mainly proposes the concept of power angle small-signal stability (PAS) as a simpler way of analyzing the small-signal stability of the VSM-controlled grid-forming inverters. This simplified method will be of great help in the future for analyzing the rotor angle small-signal stability issue of the power system when there will be large share of converter-interfaced renewable power sources. This method will save much time and computational resources by neglecting the fast dynamics of inner voltage and current control loops of the converter and only considering the power loop, where the variable power angle lies.

Based on this PAS concept and a VSM control scheme proposed earlier, the state-space representation and block diagram are derived for a system, which consists of a VSM-controlled grid-forming inverter connected to an infinite bus. This PAS model is compared with the original system with minor acceptable errors by time-domain simulations in MATLAB Simulink. Influence of the four main parameters in the power loop on the PAS of the system is investigated in detail. The conclusions are as follows.

Due to the inclusion of the governor branch in the proposed VSM control scheme, a third real eigenvalue is produced for the system, which is only influenced by the two parameters in the governor branch: the droop D_r and the response time T_g .

A larger inertia constant H reduces the stability margin, but enhances the inertia response and frequency control capability of the WT. Hence, a trade-off between both aspects needs to be considered when designing this parameter.

When designing the damping coefficient D , firstly, a range of D needs to be confirmed to guarantee the system remains stable; secondly, a trade-off also needs to be considered between stability margin and frequency control capability.

A larger droop D_r helps improving the stability, with its optimal value being more likely constraint by other factors, like rating of extra power source/sink, rating of the inverter and grid code requirements.

A smaller response time T_g helps improving the stability.

ACKNOWLEDGMENT

This work has received funding from the European Union's Horizon 2020 research and innovation program under grant agreement No. 727680 (TotalControl).

This work has also received funding from project PowerKey (EUDP Project No. 12558).

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